36. Application to some Standard Non-Correlated Pulse Train Types (Line Codes)

Here we apply our boxed results (35.17) to statistical pulse trains of various types. When a pulse train is in fact a voltage on a pair of wires (transmission line, such as a telephone "line"), the way in which signals are encoded in the pulse train is called a **line code**. One could consider a random speed Morse code signal going down a wire as a line code, but the term usually refers to a sequence of equally spaced amplitude modulated pulses, meaning a pulse train. Often line codes get modulated onto an RF carrier, in which case the line code is thought of as the baseband signal prior to modulation. For this reason, line codes are often discussed in the "baseband chapter" of any digital communications text.

The line code names are a little strange due to their history. Here are the pulse shapes used for RZ and NRZ lines codes. In either case a 1 is (is coded as) a pulse and a 0 is no pulse.

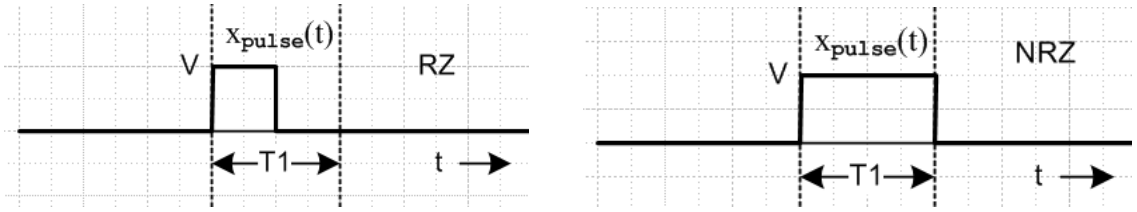


Fig 36.1

On the left, since the signal returns to zero inside the pulse period, it is called a "return to zero" code RZ. Since this does not happen on the right, that is a "non return to zero" code, NRZ.

(a) Unipolar NRZ line code

Pulse Shape. The pulse is a box of amplitude V and width $\tau = T_1$,

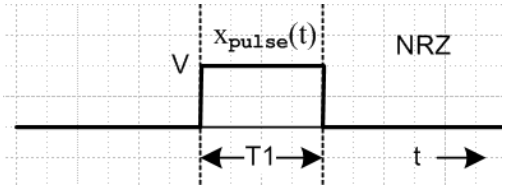


Fig 36.2

From (9.2) we know that

$$X_{pulse}(\omega) = (VT_1)\,\mathrm{sinc}(\omega T_1/2) \tag{36.1}$$

$$\mathcal{P}_{pulse}(\omega) = \frac{|X_{pulse}(\omega)|^2}{2\pi T_1} = (VT_1)^2\,\mathrm{sinc}^2(\omega T_1/2)/(2\pi T_1) = (1/2\pi)\,V^2 T_1\,\mathrm{sinc}^2(\omega T_1/2)$$

Coding: NRZ is a normal binary signal, high for period T_1 to indicate a 1, and low for T_1 to indicate a 0. Sometimes this is called unipolar NRZ since the signal never goes negative.

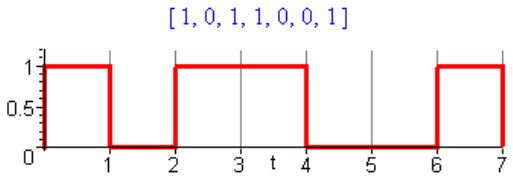


Fig 36.3

Coefficients α and β: Looking at summary box (35.17), since A = 1 and B = 0 we have $\alpha = p^2$ and $\beta = p$.

Spectrum: The average spectral power density for the NRZ line code is :

$$\langle \mathcal{P}(\omega) \rangle = \mathcal{P}_{\text{pulse}}(\omega)\,[(\beta-\alpha) + \alpha \sum_{m=-\infty}^{\infty} 2\pi\delta(\omega T_1 - 2\pi m)\,] \qquad (35.11)$$

$$= (1/2\pi)\, V^2 T_1\, \text{sinc}^2(\omega T_1/2)\,[\, p(1-p) + p^2 \sum_{m=-\infty}^{\infty} 2\pi\,\delta(\omega T_1 - 2\pi m)\,]$$

$$= (V^2/\omega_1)\, \text{sinc}^2\!\left(\pi \frac{\omega}{\omega_1}\right)[\, p(1-p) + p^2 \sum_{m=-\infty}^{\infty} \delta\!\left(\frac{\omega}{\omega_1} - m\right)\,] \ .$$

But for all m≠0, the sinc function vanishes, so the discrete part of the spectrum collapses to a single term and we get

$$\langle \mathcal{P}(\omega) \rangle = (V^2/\omega_1)\, \text{sinc}^2\!\left(\pi \frac{\omega}{\omega_1}\right)[\, p(1-p) + p^2\, \delta\!\left(\frac{\omega}{\omega_1}\right)\,]$$

From now on we shall express $\langle \mathcal{P}(\omega) \rangle$ in terms of a **dimensionless frequency** x,

$$x \equiv \frac{\omega}{\omega_1} \qquad \omega_1 \equiv 2\pi/T_1 \qquad \Rightarrow \qquad \pi x = (\omega T_1/2) \qquad (36.2)$$

so the above becomes

$$\langle \mathcal{P}(\omega) \rangle = (V^2/\omega_1)\, \text{sinc}^2(\pi x)\,[\, p(1-p) + p^2\, \delta(x)\,]$$

$$= (V^2/\omega_1)\,[p(1-p)\text{sinc}^2(\pi x) + p^2\, \delta(x)] \qquad \text{// unipolar NRZ} \qquad (36.3)$$

In order to express this (and later) results in the frequency domain, we use these relations

$\mathcal{P}(\omega) = P(f)/2\pi$ // (34.4) bottom line
$1/\omega_1 = T_1/2\pi$
$x = \omega/\omega_1 = fT_1$ // $\omega = 2\pi f$
$\delta(x) = \delta(f)/T_1$

to obtain

$$\langle P(f)\rangle = V^2\,[p(1-p)\,T_1 \mathrm{sinc}^2(\pi f T_1) + p^2\delta(f)] \qquad \text{// unipolar NRZ, f} \qquad (36.3a)$$

$$\langle P(f)\rangle = (V^2/4)[\,T_1\,\mathrm{sinc}^2(\pi f T_1) + \delta(f)\,] \qquad \text{// unipolar NRZ, f, p=1/2} \qquad (36.3b)$$

This last result agrees with Xiong (2.25).

Plot: Ignoring the overall factor (V^2/ω_1) we make this plot of $\langle \mathscr{P}(\omega)\rangle$ given by (36.3):

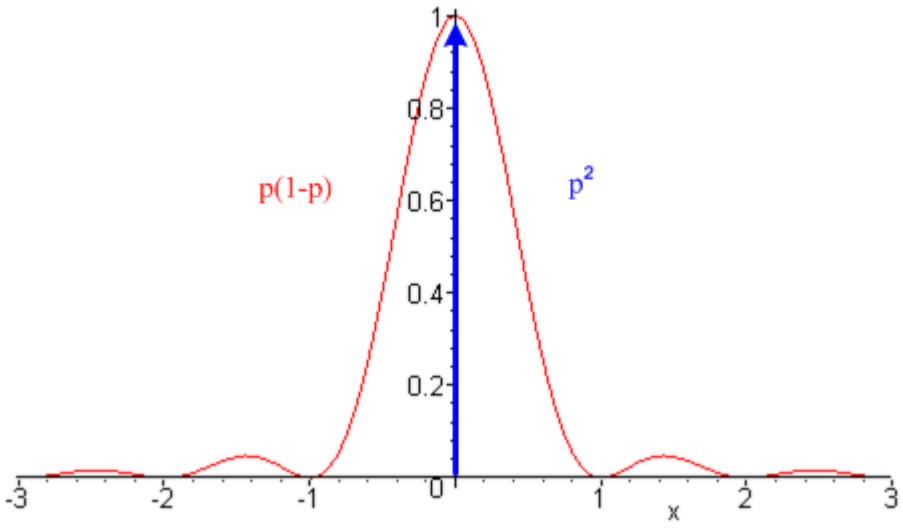


Fig 36.4

The red curve should be scaled by the red factor shown on the left, and the blue delta line should be scaled by the blue factor on the right.

Power Partition: The total power in the continuous part of the spectrum is:

$$\text{AC power} = \int_{-\infty}^{\infty} \omega_1 dx \langle \mathscr{P}(x\omega_1)\rangle = p(1-p)\,V^2 \int_{-\infty}^{\infty} dx\, \mathrm{sinc}^2(\pi x) = p(1-p)\,V^2\ .$$

The total power in the DC line at $\omega = 0$ is

$$\text{DC power} = \int_{-\infty}^{\infty} \omega_1 dx \langle \mathscr{P}(x\omega_1)\rangle = V^2 \int_{-\infty}^{\infty} dx\, p^2\,\delta(x) = p^2V^2$$

Thus we find that

$$\text{total power} = \underset{\text{DC}}{p^2\,V^2} + \underset{\text{AC}}{p(1-p)\,V^2} = pV^2 \qquad (36.4)$$

If $p = 1/2$, then

$$\text{total power} = \underset{\text{DC}}{(1/4)\,V^2} + \underset{\text{AC}}{(1/4)\,V^2} = (1/2)V^2$$

so half the power is in the DC line and half in the AC signal. The DC term is certainly reasonable since we know that with p = 1/2, the average voltage is (V/2).

If one wanted to reduce wasted power, it would be good to give this signal a DC offset of -V/2 and then there would be no DC line. This is in fact the next example if one takes V → V/2.

(b) Bipolar NRZ line code

Pulse Shape. The pulse shape is the same as for Unipolar NRZ

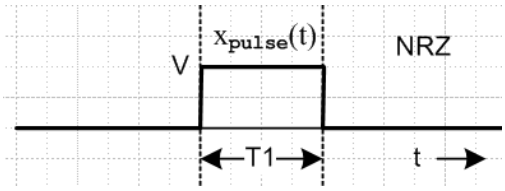


Fig 36.2

$\mathcal{P}_{pulse}(\omega) = (1/2\pi)\, V^2 T_1\, \mathrm{sinc}^2(\omega T_1/2) = (V^2/\omega_1)\, \mathrm{sinc}^2(\omega T_1/2)$ same as for unipolar NRZ *(36.1)*

Coding: 1 is coded as a positive box with amplitude V, and a 0 as a negative box having amplitude -V.

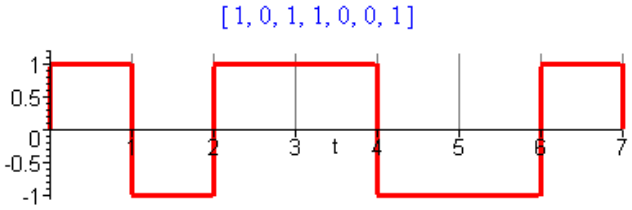


Fig 36.5

Coefficients α and β: From (35.17) we have

$\alpha = [pp]\, AA + [p(1-p)]\, AB + [(1-p)p]BA + [(1-p)(1-p)]BB$

$= [pp]\,(1)(1) + [p(1-p)]\,(1)(-1) + [(1-p)p]\,(-1)(1) + [(1-p)(1-p)]\,(-1)(-1)$

$= p^2 - 2p(1-p) + (1-p)^2 = 4p^2 - 4p + 1 = (1-2p)^2 \quad // = \mu^2$

$\beta = [p]AA + [(1-p)]\, BB = [p]\,(1)(1) + [(1-p)]\,(-1)(-1) = p + 1 - p = 1$

$(\beta - \alpha) = 1 - [4p(p-1)+1] = 4p(1-p) \quad // = \sigma^2$ (36.5)

Spectrum: The average spectral power density for the NRZ line code is :

$$\langle \mathcal{P}(x\omega_1) \rangle = \mathcal{P}_{pulse}(\omega) \left[(\beta-\alpha) + \alpha \sum_{m=-\infty}^{\infty} \delta(x - m) \right] \qquad (35.11)$$

$$= (V^2/\omega_1)\, \mathrm{sinc}^2(\pi x) \left[4p(1-p) + (1-2p)^2 \sum_{m=-\infty}^{\infty} \delta(x - m) \right] .$$

As before the sinc function kills all the δ peaks except the DC peak, so in fact

$$\langle \mathcal{P}(\omega) \rangle = (V^2/\omega_1)\,\mathrm{sinc}^2(\pi x)\,[\,4p(1-p) + (1-2p)^2\delta(x)\,] \qquad \text{// bipolar NRZ} \qquad (36.6)$$

$$\langle P(f) \rangle = (V^2 T_1)\,\mathrm{sinc}^2(\pi f T_1)\,[\,4p(1-p) + (1-2p)^2\delta(f)/T_1\,] \qquad \text{// bipolar NRZ, f} \qquad (36.6a)$$

$$\langle \mathcal{P}(\omega) \rangle = (V^2/\omega_1)\,\mathrm{sinc}^2(\pi x) = \mathcal{P}_{\mathtt{pulse}}(\omega) \qquad \text{// bipolar NRZ, p=1/2} \qquad (36.6b)$$

$$\langle P(f) \rangle = (V^2 T_1)\,\mathrm{sinc}^2(\pi f T_1) \qquad \text{// bipolar NRZ, f, p = 1/2} \qquad (36.6c)$$

This last result agrees with Xiong (2.20). The spectrum is all continuous when p = 1/2 since then the DC portion is killed off. As noted in the comment after (35.11a), a discrete spectrum cannot exist if the waveform amplitudes have zero mean μ = 0.

Notice that for p = 1/2, bipolar NRZ has $\langle \mathcal{P}(\omega) \rangle = \mathcal{P}_{\mathtt{pulse}}(\omega)$, so the statistical pulse train spectrum is the same as that of the underlying pulse.

Plot: Ignoring the overall factor (V^2/ω_1) we make this plot of $\langle \mathcal{P}(x\omega_1) \rangle$ given by (36.6)

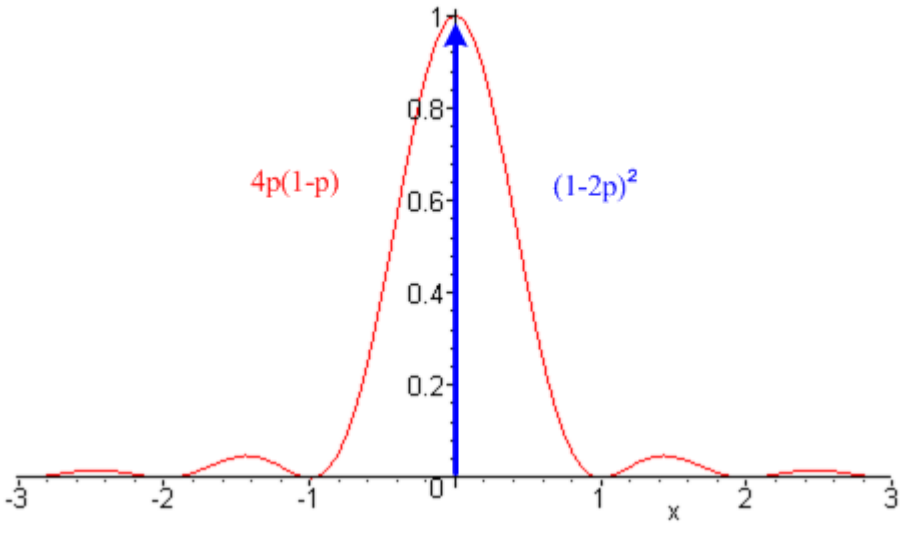


Fig 36.6

which is the same as the spectrum for unipolar NRZ except for the two scaling factors.

Power Partition: We can again compute the DC and AC power.

AC power = unipolar NRZ with $p(1-p) \rightarrow 4p(1-p)$, so AC = $4p(1-p)\,V^2$

DC power = unipolar NRZ with $p^2 \rightarrow (2p-1)^2$, so DC = $(2p-1)^2\,V^2$

$$\text{total power} = \underset{\text{DC}}{(2p-1)^2V^2} + \underset{\text{AC}}{4p(1-p)V^2} = V^2 \quad \text{, independent of p.} \qquad (36.7)$$

The total power is independent of p because a pulse has the same AC power if it goes up or down. For p = 1/2 we get

$$\text{total power} = \underset{\text{DC}}{0} + \underset{\text{AC}}{V^2} = V^2 \qquad \text{// } p = 1/2$$

and now no power is wasted pushing DC through a line. If we take V→V/2 to have a comparable peak-to-peak amplitude, we find

$$\text{AC power} = (V/2)^2$$

which is the same as the AC power in (36.5); it is not affected by a DC offset of -V/2.

(c) Unipolar RZ line code

Pulse Shape. Here the basic pulse is a box that fills only half the time interval T_1.

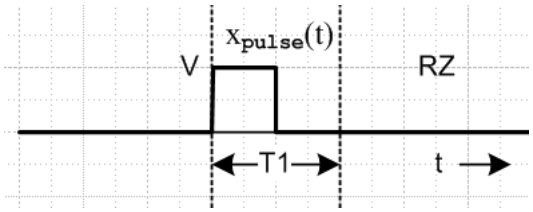


Fig 36.7

We can use result (36.1) with $T_1 \rightarrow T_1/2$ since the pulse only fills half the T_1 period,

$$X_{pulse}(\omega) = (VT_1/2)\,\text{sinc}(\omega T_1/4)$$

$$\mathcal{P}_{pulse}(\omega) = \frac{|X_{pulse}(\omega)|^2}{2\pi T_1} = (VT_1/2)^2\,\text{sinc}^2(\omega T_1/4)/(2\pi T_1) = (1/2\pi)\,(V/2)^2 T_1\,\text{sinc}^2(\omega T_1/4)$$

$$= (V/2)^2\,(1/\omega_1)\,\text{sinc}^2\left(\frac{\pi}{2}\frac{\omega}{\omega_1}\right) \qquad (36.8)$$

Coding: 1 is coded as the presence of the pulse, 0 is coded as the absence of a pulse.



Fig 36.8

Coefficients α and β: Looking at summary box (35.17), since A = 1 and B = 0 we have $\alpha = p^2$ and $\beta = p$.

Spectrum: The average spectral power density for the unipolar RZ line code is :

$$\langle \mathcal{P}(\omega) \rangle = \mathcal{P}_{\text{pulse}}(\omega)\,[(\beta-\alpha) + \alpha \sum_{m=-\infty}^{\infty} 2\pi\delta(\omega T_1 - 2\pi m)\,]$$

$$= (V/2)^2\,(1/\omega_1)\,\text{sinc}^2\!\left(\frac{\pi}{2}\frac{\omega}{\omega_1}\right)[\,p(1-p) + p^2 \sum_{m=-\infty}^{\infty} \delta\!\left(\frac{\omega}{\omega_1} - m\right)\,]$$

$$= (V/2)^2\,(1/\omega_1)\,\text{sinc}^2\!\left(\frac{\pi}{2}x\right)[\,p(1-p) + p^2 \sum_{m=-\infty}^{\infty} \delta(x - m)\,]\ .$$

We see here that the sinc function now kills off all m= even lines for m ≠0, so with x = ω/ω1,

$$\langle \mathcal{P}(\omega) \rangle = (V/2)^2\,(1/\omega_1)\,\text{sinc}^2\!\left(\frac{\pi}{2}x\right)[\,p(1-p) + p^2\,\{\delta(x) + \sum_{m\ \text{odd}} \delta(x - m)\}\,] \qquad (36.9)$$

$$\langle P(f) \rangle = (V/2)^2 T_1\,\text{sinc}^2\!\left(\frac{\pi}{2}fT_1\right)[\,p(1-p) + (p^2/T_1)\,\{\delta(f) + \sum_{m\ \text{odd}} \delta(f - m/T_1)\,\}\,] \qquad (36.9a)$$

where the sum includes positive and negative odd values of m. As noted above, one can formally include the even m terms but they vanish since sinc(mπ/2) = 0 for even m ≠ 0. For p = 1/2 one gets

$$\langle P(f) \rangle = (V/4)^2 T_1\,\text{sinc}^2\!\left(\frac{\pi}{2}fT_1\right)[\,1 + (1/T_1)\,\{\delta(f) + \sum_{m\ \text{odd}} \delta(f - m/T_1)\,\}\,]$$

$$= (V/4)^2 T_1\,\text{sinc}^2\!\left(\frac{\pi}{2}fT_1\right)[\,1 + (1/T_1) \sum_{m=-\infty}^{\infty} \delta(f - m/T_1)\,] \qquad \text{// } p = 1/2 \qquad (36.9b)$$

This last result agrees with Xiong (2.31) in which $R_b \equiv 1/T$ = our $1/T_1$.

Plot: Ignoring now the overall factor $(V/2)^2\,(1/\omega_1)$ we get this power spectrum from (36.9),

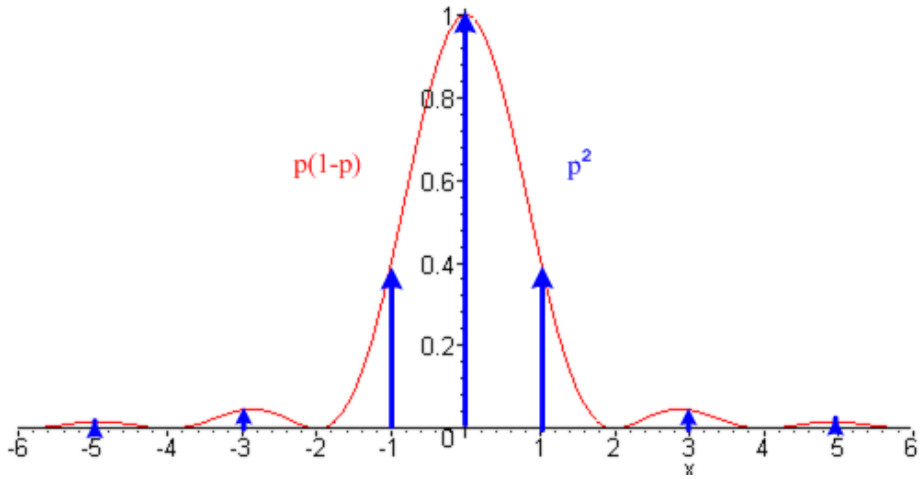


Fig 36.9

We now have three pieces: a continuous part, the DC line, and a set of lines at odd m. The main peak is twice as wide as the NRZ peak since the underlying pulse is half as wide.

Power Partition: Once again, we can compute the total power for each of these three pieces.

$$\text{odd lines power} = \int_{-\infty}^{\infty} \omega_1 dx \langle \mathcal{P}(x\omega_1) \rangle = \omega_1 (V/2)^2 (1/\omega_1) p^2 \int_{-\infty}^{\infty} dx \, \text{sinc}^2\left(\frac{\pi}{2} x\right) 2 \sum_{m = 1\,3\,5\ldots}^{\infty} \delta(x - m)$$

$$= (V/2)^2 2p^2 \sum_{m = 1\,3\,5\ldots}^{\infty} \text{sinc}^2\left(\frac{\pi}{2} m\right) = (V/2)^2 2p^2 \sum_{m = 1\,3\,5\ldots}^{\infty} \frac{\sin^2\left(\frac{\pi}{2} m\right)}{\left(\frac{\pi}{2} m\right)^2} = (V/2)^2 2p^2 (2/\pi)^2 \sum_{m = 1\,3\,5\ldots}^{\infty} \frac{1}{m^2}$$

$$= (V/2)^2 2p^2 (2/\pi)^2 (\pi^2/8) = p^2 (V/2)^2$$

where the sum $\Sigma_{\text{odd}}(1/m^2) = \pi^2/8$ from GR 0.234.2. Then

$$\text{DC power} = \int_{-\infty}^{\infty} \omega_1 dx \langle \mathcal{P}(x\omega_1) \rangle = (V/2)^2 p^2 \int_{-\infty}^{\infty} dx \, \text{sinc}^2\left(\frac{\pi}{2} x\right) \delta(x) = p^2 (V/2)^2$$

which is the same as the odd lines power. Finally,

$$\text{continuum power} = \int_{-\infty}^{\infty} \omega_1 dx \langle \mathcal{P}(x\omega_1) \rangle = (V/2)^2 p(1-p) \int_{-\infty}^{\infty} dx \, \text{sinc}^2\left(\frac{\pi}{2} x\right) = 2p(1-p) (V/2)^2$$

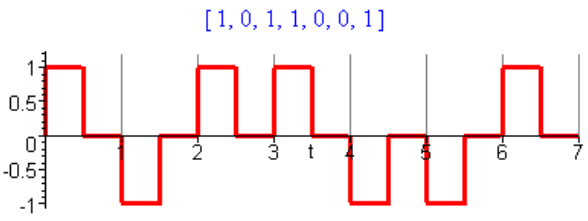
So the power partitioning is

$$\text{total power} = \underbrace{p^2(V/2)^2}_{\text{DC}} + \underbrace{p^2 (V/2)^2}_{\text{other lines}} + \underbrace{2p(1-p) (V/2)^2}_{\text{continuum}}$$

$$= \underbrace{p^2(V/2)^2}_{\text{DC}} + \underbrace{p(2-p) (V/2)^2}_{\text{AC}} = 2p(V/2)^2 = (p/2)V^2 \, . \qquad (36.10)$$

This is half of the total power of unipolar NRZ (36.4), which seems reasonable since the pulses here are half as long.

Exercise for the Reader: Compute everything for the bipolar RZ waveform:



For p = 1/2, Xiong (2.30) gives $\langle P(f) \rangle = (V/2)^2 T_1 \, \text{sinc}^2\left(\frac{\pi}{2} f T_1\right)$.

(d) Manchester line code

This line code was developed at the University of Manchester probably in the World War II era. At that time Tom Kilburn, Alan Turing and others were building the world's first stored-program computer.

Pulse Shape: The pulse shape here is the biphase (biphasic, diphase) pulse,

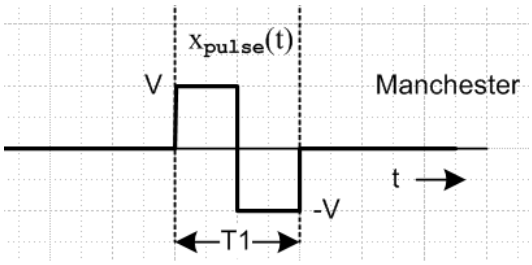


Fig 36.10

We already computed $X_{pulse}(\omega)$ for this pulse in (19.2), so we now set $\tau = T_1/2$ and $A/2 = V$ to get

$$X_{pulse}(\omega) = (4iV/\omega)\sin^2(\omega T_1/4) = (4iV/\omega)\sin(\omega T_1/4)\,[\sin(\omega T_1/4)/(\omega T_1/4)]\,(\omega T_1/4)$$

$$= (iVT_1)\sin(\omega T_1/4)\,\mathrm{sinc}(\omega T_1/4)$$

$$\mathcal{P}_{pulse}(\omega) = \frac{|X_{pulse}(\omega)|^2}{2\pi T_1} = (1/2\pi)\,V^2\,T_1\sin^2(\omega T_1/4)\,\mathrm{sinc}^2(\omega T_1/4)\ . \qquad (36.11)$$

This spectral pulse density is $4\sin^2(\omega T_1/4)$ times that of the RZ pulse shown in (36.8). This extra factor kills off the spectrum near $\omega = 0$.

Coding: 1 is coded as the above pulse, 0 is coded as the negative of the pulse (but some sources use the opposite polarity),

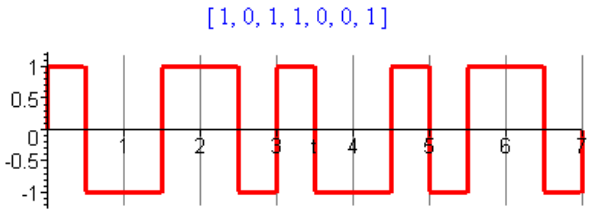


Fig 36.11

Coefficients α and β: From box (35.17) with A = 1 and B = -1,

$$\alpha = [pp]\,AA + [p(1-p)]\,AB + [(1-p)p]BA + [(1-p)(1-p)]BB$$
$$= [pp]\,(1)(1) + [p(1-p)]\,(1)(-1) + [(1-p)p]\,(-1)(1) + [(1-p)(1-p)]\,(-1)(-1)$$
$$= p^2 - 2p(1-p) + (1-p)(1-p) = (2p-1)^2$$

$$\beta = [p]AA + [(1-p)]\,BB = [p]\,(-1)(-1) + [(1-p)]\,(1)(1) = 1$$

$$(\beta-\alpha) = 1 - (2p-1)^2 = 4p(1-p) \qquad (36.12)$$

Comment: Notice that the mean value of the waveform in Fig 36.11 is 0 regardless of p, whereas the mean value μ of the amplitudes y_n is given by $\mu^2 = \alpha = (2p-1)^2$ as in (D.17).

Spectrum: The average spectral power density for the Manchester line code is :

$$\langle \mathcal{P}(\omega) \rangle = \mathcal{P}_{pulse}(\omega)\,[(\beta-\alpha) + \alpha \sum_{m=-\infty}^{\infty} 2\pi\delta(\omega T_1 - 2\pi m)\,]$$

$$= (1/2\pi)\, V^2\, T_1 \sin^2(\omega T_1/4)\, \mathrm{sinc}^2(\omega T_1/4)\,[4p(1-p) + (2p-1)^2 \sum_{m=-\infty}^{\infty} 2\pi\delta(\omega T_1 - 2\pi m)$$

$$= V^2\,(1/\omega_1)\, T_1 \sin^2\!\left(\frac{\pi}{2}\frac{\omega}{\omega_1}\right) \mathrm{sinc}^2\!\left(\frac{\pi}{2}\frac{\omega}{\omega_1}\right)\,[4p(1-p) + (2p-1)^2 \sum_{m=-\infty}^{\infty} \delta\!\left(\frac{\omega}{\omega_1} - m\right)\,]$$

$$= V^2\,(1/\omega_1) \sin^2\!\left(\frac{\pi}{2}x\right) \mathrm{sinc}^2\!\left(\frac{\pi}{2}x\right)\,[4p(1-p) + (2p-1)^2 \sum_{m=-\infty}^{\infty} \delta(x - m)\,]$$

so that

$$\langle \mathcal{P}(\omega) \rangle = V^2\,(1/\omega_1) \sin^2\!\left(\frac{\pi}{2}x\right) \mathrm{sinc}^2\!\left(\frac{\pi}{2}x\right)\,[4p(1-p) + (2p-1)^2 \sum_{m=\pm\mathrm{odd}} \delta(x - m)\,] \qquad (36.13)$$

$$\langle P(f) \rangle = V^2 T_1 \sin^2\!\left(\frac{\pi}{2} f T_1\right) \mathrm{sinc}^2\!\left(\frac{\pi}{2} f T_1\right)\,[4p(1-p) + (2p-1)^2 (1/T_1) \sum_{m=\pm\mathrm{odd}} \delta(f - m/T_1\,] \qquad (36.13a)$$

$$\langle P(f) \rangle = V^2 T_1 \sin^2\!\left(\frac{\pi}{2} f T_1\right) \mathrm{sinc}^2\!\left(\frac{\pi}{2} f T_1\right) \qquad // \; p = 1/2 \qquad (36.13b)$$

For p≠1/2, the even lines are killed off by the $\sin^2$ factor including the DC line m = 0. For p = 1/2 the spectrum is fully continuous. The last result agrees with Xiong (2.38). Xiong refers to this Manchester code as Bi-Φ-L.

Plot: Ignoring the leading factor $V^2\,(1/\omega_1)$ the spectrum for (36.13) has this plot,

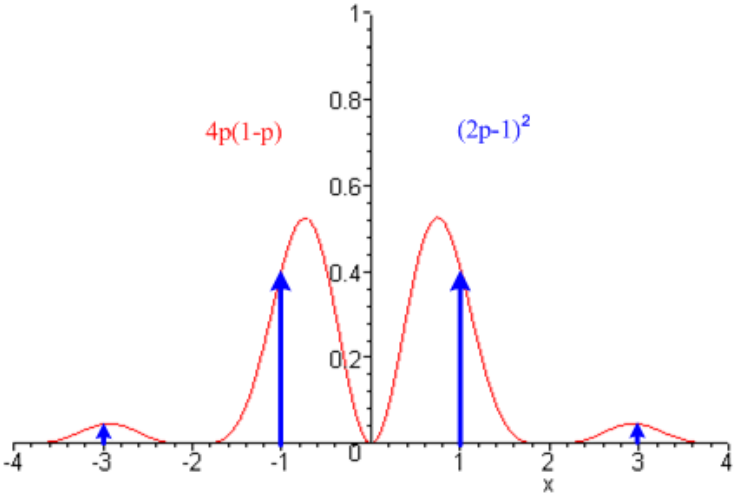


Fig 36.12

Power Partition:

$$\text{lines power} = \int_{-\infty}^{\infty} \omega_1 dx \langle \mathcal{P}(x\omega_1) \rangle = V^2 (2p-1)^2 \int_{-\infty}^{\infty} dx \sin^2(\frac{\pi}{2}x) \operatorname{sinc}^2(\frac{\pi}{2}x) \sum_{m = \pm\text{odd}} \delta(x - m)$$

$$= V^2 (2p-1)^2 \sum_{m = \pm\text{odd}} \sin^2(\frac{\pi}{2}m) \operatorname{sinc}^2(\frac{\pi}{2}m) = V^2 (2p-1)^2 \sum_{m = \pm\text{odd}} \sin^4(\frac{\pi}{2}m) (\frac{\pi}{2}m)^{-2}$$

$$= V^2 (2p-1)^2 (2/\pi)^2 \sum_{m = \pm\text{odd}} 1/m^2 = V^2 (2p-1)^2 (2/\pi)^2 \, 2 \sum_{m = 1\,3\,5\ldots}^{\infty} 1/m^2$$

$$= V^2 (2p-1)^2 (2/\pi)^2 \, 2 \, (\pi^2/8) = (2p-1)^2 V^2$$

$$\text{continuum power} = \int_{-\infty}^{\infty} \omega_1 dx \langle \mathcal{P}(x\omega_1) \rangle = V^2 \, 4p(1-p) \int_{-\infty}^{\infty} dx \sin^2(\frac{\pi}{2}x) \operatorname{sinc}^2(\frac{\pi}{2}x) = V^2 \, 4p(1-p)$$

since the integral is just 1. Therefore,

$$\text{total power} = \underset{\text{DC}}{0} + \underset{\text{lines}}{(2p-1)^2 V^2} + \underset{\text{continuum}}{4p(1-p) V^2} = \underset{\text{AC}}{V^2} \qquad (36.14)$$

In the case p = 1/2, the lines power vanishes leaving only continuum power = V^2.

Since the power is kept away from DC, Manchester coding is useful for AC-coupled transmission lines, such as lines incorporating transformers. The down side compared to NRZ is that the first spectral hump goes out to $\omega = 2\omega_1$, which reflects the fact that the minimum pulse width is $T_1/2$ whereas in NRZ it is T_1. So a transmission line must then have twice the bandwidth for Manchester relative to NRZ.

(e) Noise, ISI and Eye Patterns

In general, if some spectral components are filtered away in a transmission line (or in some general signal pathway), the corresponding pulse (by inverse Fourier Transform) has curved corners, meaning the pulse gets rounded and spread out. This effect along with noise can result in **inter-symbol interference (ISI)**. The superposition of such pulses on an oscilloscope (triggered on a recovered T_1 clock) for a random pulse train is called an **eye pattern.** This pattern must have a central clear area to allow the two (or more for some line codes) pulse levels to be distinguished by a receiving circuit. Here is a marginal eye pattern for NRZ on the left, and a better one for AMI on the right (see Section 37).

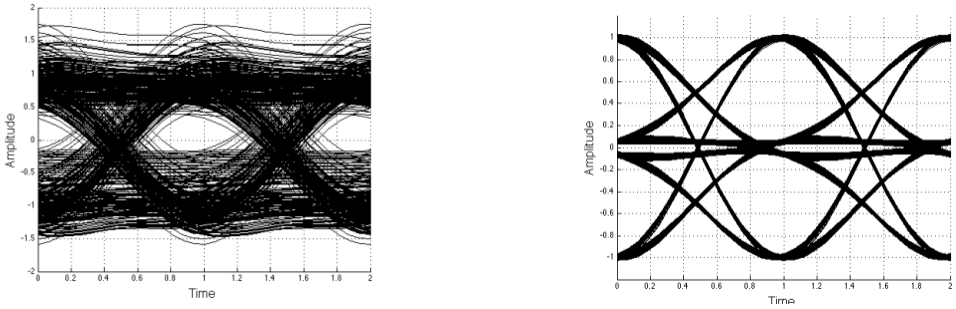


Fig 36.13